A Discussion of an Analytical Per-Unit-Length Impedance Matrix Model

Frédéric Broydé and Evelyne Clavelier
Tekcem
12 chemin des Hauts de Clairefontaine, 78580 Maule, France
e-mail: {fredbroyde,eclavelier}@tekcem.com

Abstract — An analytical model for the per-unit-length impedance matrix of a multiconductor interconnection has recently been introduced and shown to be physically reasonable. The present discussion addresses the determination of the model parameters and the model accuracy.

Keywords — Multiconductor transmission lines, resistive loss model, signal integrity analysis.

I. INTRODUCTION

This paper relates to an analytical model for the per-unit-length (p.u.l.) impedance matrix of a multiconductor interconnection having \( n \) transmission conductors (TCs) and a reference conductor (GC), such as the structures shown in Fig. 1 and Fig. 2. The p.u.l. impedance matrix is a frequency dependent complex \( n \times n \) matrix denoted by \( Z' \). It may be split into two terms:

\[
Z' = Z_0' + j \omega L_0'
\]  

(1)

where \( \omega \) is the radian frequency, \( L_0' \) is a frequency independent real \( n \times n \) matrix sometimes referred to as the p.u.l. external inductance matrix, or more precisely as the high-frequency p.u.l. external inductance matrix and \( Z_0' \) is a frequency dependent complex \( n \times n \) matrix traditionally referred to as the p.u.l. internal impedance matrix. \( L_0' \) is the p.u.l. inductance matrix computed at a non-zero frequency under the assumption that all conductors of the interconnection are ideal conductors, i.e., lossless conductors. It is usually determined using the relation \( L_0' = \mu_0/\varepsilon_0 C_0^{-1} \), where \( \mu_0 \) is the permeability of vacuum, \( \varepsilon_0 \) is the permittivity of vacuum and \( C_0^{-1} \) is the p.u.l. capacitance matrix of an interconnection obtained from the original interconnection by replacing the dielectrics with vacuum and the conductors with ideal conductors having the same geometry. Here, \( Z_0' \) is defined by (1). Thus, (1) is exact and writing the imaginary part \( Z_j' \) in the form \( \Im(Z_j') = j\omega L_j' \) defines \( L_j' \) as an incremental inductance instead of an internal inductance determined by the average magnetic energy within the conductors [1].

For non-magnetic conductors having a homogeneous cross-section and no surface roughness, an analytical model for \( Z_j' \), denoted by \( Z_j'_{\text{xy}} \), has recently been proposed [2]. At high frequency (h.f.), it takes into account a normal skin effect, the crowding of currents at the edges of the conductors (edge effect), and the interaction between the current distributions on different conductors (proximity effect). It was shown that this analytical model is physically reasonable and realizable in the sense that it is accurate at dc and h.f., corresponds to a finite dc inductance matrix, and that it represents a causal and passive linear system. Replacing \( Z_j' \) in (1) with \( Z_j'_{\text{xy}} \) produces the analytical p.u.l. impedance matrix model discussed in this paper.

This model is briefly presented in Section II. The determination of some of the model parameters is discussed in Section III. In Section IV, we compute the model parameters for two interconnections and we compare the impedance matrix predicted by the model with an impedance matrix computed using the differential surface admittance operator technique [1] [3].

II. PRESENTATION OF THE \( Z_j'_{\text{xy}} \) MODEL

We assume that all TCs have the same homogeneous resistivity \( \rho_{\text{TC}} \) and that the GC has an homogeneous resistivity \( \rho_{\text{GC}} \). The matrix of the equivalent inverse widths of the TCs, denoted by \( K_{TC} \), and the matrix of the equivalent inverse widths of the GC, denoted by \( K_{GC} \), can be determined at a low computational cost [4] [5]. \( K_{TC} \) and \( K_{GC} \) are frequency independent, real and positive semidefinite \( n \times n \) matrices. The \( Z_j'_{\text{xy}} \) model is defined by...
\[
Z'_N = Z'_{NR} + Z'_{NTC} + Z'_{NGC}
\]

where, for the indices \( \alpha \) and \( \beta \) ranging from 1 to \( n \) with \( \alpha \neq \beta \), the entries of the matrices \( Z'_{NR} \), \( Z'_{NTC} \) and \( Z'_{NGC} \) are given by

\[

Z'_{NR\alpha\beta} = \frac{R'_{DCA} + R'_{DCG}}{1 + \frac{4sL_N^{2\text{NGC}}}{\mu_0 \rho_{GC} (\max_{\gamma\alpha\alpha} K_{GC\gamma})^2}}
\]

\[
Z'_{NTC\alpha\beta} = \frac{\mu_0 \rho_{TC} K_{TC\alpha}}{2L_{\text{MAX}}^a} \left( 1 + \frac{4sL_N^{2\text{MAX}}}{\mu_0 \rho_{TC} K_{TC\alpha}} - 1 \right)
\]

\[
Z'_{NGC\alpha\beta} = \frac{\mu_0 \rho_{GC} K_{GC\alpha}}{2L_{\text{MAX}}^G} \left( \frac{L_N^{\text{MAX}}}{K_{TC\alpha}} \right) \left( \frac{L_N^{\text{MAX}}}{K_{TC\beta}} \right) - 1
\]

\[
Z'_{NGC} = \frac{\mu_0 \rho_{GC} K_{GC\alpha}}{2L_{\text{MAX}}^G} \left( 1 + \frac{4sL_N^{2\text{MAX}}}{\mu_0 \rho_{GC} (\max_{\gamma\alpha\alpha} K_{GC\gamma})^2} - 1 \right) K_{GC}
\]

where \( s \) is the Laplace transform variable, where each square root symbol denotes the principal root, where the p.u.l. dc resistances of the TCs are denoted by \( R'_{DC1} \) to \( R'_{DCn} \), and where the p.u.l. resistance \( R'_{DCG} \) and the p.u.l. inductances \( L'_{MAX1} \) to \( L'_{MAXn} \), \( L'_{NEGGC} \) and \( L'_{MAXGC} \) are positive parameters.

At frequencies high enough for the skin effect to be well developed, the largest contribution to \( Z'_N \) comes from \( Z'_{NTC} \) and \( Z'_{NGC} \) and the \( 1 \) are negligible in (4) and (5). Thus, the parameters controlling the h.f. behavior of the model are \( \rho_{TC} \), \( \rho_{GC} \), \( K_{TC} \) and \( K_{GC} \). Conversely, the dc value of \( Z'_N \) is a resistance matrix solely determined by \( Z'_{NR} \). It may be easily verified that \( Z'_{NR} \), \( Z'_{NTC} \) and \( Z'_{NGC} \) contribute to the dc inductance matrix. The main motivation for introducing the \( Z'_N \) model is that all entries of the dc inductance matrix are finite, unlike the dc inductance matrix of a model in the form \( Z'_S = A + s^{1/2} B \) where \( A \) and \( B \) are two frequency independent matrices. The parameters \( R'_{DC1} \) to \( R'_{DCn} \) of \( Z'_{NR} \) are unambiguously defined above, but not the parameters \( R'_{DCG} \), \( L'_{MAX1} \) to \( L'_{MAXn} \), \( L'_{NEGGC} \) and \( L'_{MAXGC} \). They will be further discussed in the Section III and IV.

It was observed that \( K_{TC} \) is strictly diagonally dominant. Using this result, it was proved that the impedance matrices \( Z'_{S} \), \( Z'_{NR} \), \( Z'_{NTC} \) and \( Z'_{NGC} \) each represents a passive linear system, and consequently a causal system [2]. In [2], it was assumed that \( L'_{NEGGC} = L'_{MAXGC} \) - but this assumption has been removed in (3). This has no impact on the passivity of \( Z'_{S} \), \( Z'_{NR} \), \( Z'_{NTC} \) and \( Z'_{NGC} \). \( L'_{NEGGC} \) controls a possible decrease of low frequency mutual impedances, caused by the proximity effect.
a finite value of $h$, for the main objective of minimizing the error on the diagonal entries $R' = \text{Re}(Z')$ at intermediate frequencies; $R'_{DCGC}$ should be the actual dc resistance of the GC.

IV. TWO EXAMPLES

A first example relates to the multiconductor microstrip interconnection defined above, in the case $b = 1350 \mu m$. In Fig. 3, we see that all entries of $L'_{DC}$ are positive in this case. Fig. 4 and Fig. 5 show some entries of $R'$ and $L' = \text{Im}(Z')/\omega$ according to the $Z'_{N}$ model and to an accurate numerical computation using the differential surface admittance operator technique [1] [3]. For $R'$, we observe a good agreement at every frequency and an excellent agreement at every frequency except in the intermediate frequency range from 200 kHz to 100 MHz. For $L'$, we observe a good agreement except at frequencies below 500 kHz, but this discrepancy cannot lead to a significant error in a simulation involving an on-board, on-package, or on-chip interconnections.

A second example relates to the multiconductor stripline
interconnection shown in Fig. 2, in the case \( t = h = a = w_1 = w_2 = d_1 = d_2 = 50 \mu m \) and \( b = 1350 \mu m \). Here all entries of \( \mathbf{L}'_{DC} \) are positive, except \( \mathbf{L}'_{DC14} \) and \( \mathbf{L}'_{DC41} \). Fig. 6 shows some entries of \( \mathbf{R}' \) according to the \( \mathbf{Z}'_N \) model and to the same numerical computation as above. The numerical model predicts a non-increasing frequency dependence for \( \mathbf{R}'_{14} \) below about 35 MHz. Since such a complicated behavior is not described in the literature, we performed an independent verification using a 2-D code based on the method of filaments, up to 10 MHz, for which we obtained the same result. A good agreement between the \( \mathbf{Z}'_N \) models and the numerical computation is obtained only for the diagonal entries of \( \mathbf{R}' \) and for the non-diagonal entries of \( \mathbf{R}' \) exceeding about 2 \( \Omega/m \). However, the error observed for the non-diagonal entries of \( \mathbf{R}' \) corresponds to negligible losses compared to the losses caused by the diagonal entry of \( \mathbf{R}' \).

In both examples, at every frequency, the maximum column sum matrix norm and the maximum row sum matrix norm of the error in \( \mathbf{R}' \) are small compared to the corresponding norm of \( \mathbf{R}' \), and very small except in an intermediate frequency range.

In both examples, the \( \mathbf{Z}'_N \) model uses \( \mathbf{L}'_0 \), \( \mathbf{K}_{TC} \) and \( \mathbf{K}_{GC} \) given in § VII of [5], computed for \( b = \infty \). It uses the values of \( L_{\text{MAX1}} \) to \( L_{\text{MAX}_n} \), \( L'_{\text{NEGGC}} \) and \( L'_{\text{MAXGC}} \) produced by an optimization process in which the objective function is a linear combination of squared errors of entries of \( \mathbf{R}' \) at different frequencies. For Fig. 4 and Fig. 5, we have used \( L'_{\text{MAX1}} = L'_{\text{MAX}_4} = 76.38 \text{nH/m} \), \( L'_{\text{MAX2}} = L'_{\text{MAX}_3} = 88.00 \text{nH/m} \), \( L'_{\text{NEGGC}} = 67.57 \text{nH/m} \) and \( L'_{\text{MAXGC}} = 134.28 \text{nH/m} \). For Fig. 6, we have used \( L'_{\text{MAX1}} = L'_{\text{MAX}_4} = 64.73 \text{nH/m} \), \( L'_{\text{MAX2}} = L'_{\text{MAX}_3} = 71.35 \text{nH/m} \), \( L'_{\text{NEGGC}} = 55.21 \text{nH/m} \) and \( L'_{\text{MAXGC}} = 146.99 \text{nH/m} \).

V. CONCLUSION

We have used an analytical and physically reasonable p.u.l. impedance matrix model of a multiconductor interconnection, presenting two differences with the approach used in [2]: a new parameter has been introduced and a least square error optimization was used to obtain \( L'_{\text{MAX}_1} \) to \( L'_{\text{MAX}_n} \), \( L'_{\text{NEGGC}} \) and \( L'_{\text{MAXGC}} \). The values obtained for \( L'_{\text{MAX}_1} \) to \( L'_{\text{MAX}_n} \) and \( L'_{\text{MAXGC}} \) show that they cannot be regarded as dc internal inductances, which are less than 48.32 nH/m for any rectangular conductor [8].

The \( \mathbf{Z}'_N \) model used in this paper has a small number of real and frequency independent parameters, but it provides a good accuracy for the types of interconnections that we have considered.

REFERENCES